

**INTERMODULATION DISTORTION IDENTIFICATION AND
QUANTIZATION CIRCUIT FOR A LINEAR AMPLIFIER SYSTEM**

Field of the Invention

This invention relates to the field of linear amplifiers, and more particularly, this invention relates to a method and circuit for canceling intermodulation distortion in multiple carrier linear amplifiers.

Background of the Invention

Radio frequency amplifiers use linear amplifiers that are not always "clean," and in operation, often produce intermodulation distortion. This distortion creates interference at the operating frequencies used by radio frequency, cellular, and other similar communications circuits. As cellular and other communication systems become more important and prevalent, it is necessary to reduce the intermodulation distortion produced in amplifier systems, and especially linear power amplifiers, which play an important part in these systems.

Some prior art techniques suppress intermodulation distortion by generating an inverse distortion signal and applying it to the input end of the amplifier. Another prior art technique uses a negative feedback system for negatively feeding back the distortion signals with an output signal at its input end. Other prior art techniques use a feed forward system that extracts the intermodulation

distortion signals, and inverts the phase of those signals to cancel the problematic signals. This type of system is widely used in base stations, satellites, and mobile communication systems. This system has high
5 efficiency in suppressing the signals as compared to other types of linear power amplifiers, but is typically complex in structure and large. Sometimes the circuits cause increased power losses. Decreasing intermodulation distortion becomes even more important
10 in multiple carrier linear amplifiers that are operative with multiple carriers in communications systems. Even small amounts of intermodulation distortion can create extreme performance problems.

15

Summary of the Invention

A method of the present invention is associated with a multiple carrier linear amplifier circuit and reduces intermodulation distortion by sampling the output of the multiple carrier linear
20 amplifier radio frequency signal and detecting the sampled signal at frequency increments and quantizing and nulling the intermodulation distortion. The circuit can generate a local oscillator signal having predetermined frequency increments $F_0 \dots F_i$ situated in
25 at least one of predetermined sub-bands. The sampled radio frequency signal is mixed with the local oscillator signal to target the centers of the multiple carriers and generate an intermediate frequency signal. This signal is detected and digitized for quantization
30 and nulling of the intermodulation distortion.

The method can also include the step of filtering the resultant intermediate frequency signal before detecting and digitizing for quantization. The circuit is stepped for the local oscillator frequency
35 increments $F_0 \dots F_i$ and the outputs of the stepping

operation are compared to identify sub-bands. The circuit identifies which frequencies are active in which sub-bands, and adjusts the local oscillator frequency based on determined active frequencies. The 5 generated frequency increments $F_0 \dots F_{11}$ can be incremented in five MHz increments. The radio frequency signal can be generated in the radio frequency range from about 2110 to about 2170 MHz. The radio frequency signal can be divided into three 10 sub-bands, each sub-band having up to four carriers. The intermediate frequency signal can be detected within a sample and hold circuit having a detector operative therewith.

15 **Brief Description of the Drawings**

Other objects, features and advantages of the present invention will become apparent from the detailed description of the invention which follows, when considered in light of the accompanying drawings 20 in which:

FIG. 1 is a circuit of an intermodulation distortion nulling circuit that isolates amplifier output by subtracting the clean signal from the distorted output signal while using a large delay line.

25 FIG. 2 is an alternate and improved intermodulation distortion nulling circuit of the present invention where the output of the amplifier system is used to extract the required intermodulation distortion information.

30 FIG. 3 is a circuit diagram of the intermodulation distortion identification and quantization circuit shown in FIG. 2.

FIGS. 4-9 illustrate various sub-bands relative to the ACP/AACP thresholds for different 35 carriers.

03262734 03262735

FIG. 10 is a high level flow chart illustrating an example of the algorithm that can be used for the intermodulation distortion nulling circuit of the present invention shown in FIG. 2.

5

Detailed Description of the Preferred Embodiments

The present invention will now be described more fully hereinafter with reference to the accompanying drawings, in which preferred embodiments 10 of the invention are shown. This invention may, however, be embodied in many different forms and should not be construed as limited to the embodiments set forth herein. Rather, these embodiments are provided so that this disclosure will be thorough and complete, 15 and will fully convey the scope of the invention to those skilled in the art. Like numbers refer to like elements throughout.

FIG. 1 illustrates a first intermodulation distortion nulling circuit **18** as part of a multiple 20 carrier linear amplifier (MCLA) that isolates the amplifier output intermodulation distortion and subtracts the clean input signal from the distorted output signal, thus retrieving the intermodulation distortion products. For purposes of description, the 25 general connections among components is first described, followed by a brief working of the circuit. Further details of this type of circuit are described in U.S. Patent application No. 09/564,321 filed May 3, 2000, as docket number Hoffmann 2, the disclosure which 30 is hereby incorporated by reference in its entirety.

The circuit works with a carrier cancellation loop. The circuit shown in FIG. 1 uses a large delay line, DelayS, to achieve linear operation across a wide frequency band application. This delay line 35 significantly increases the weight and cost of a multi-

DRAFTS
2004
1000
0000
0000
0000
0000
0000
0000

channel, i.e., multiple carrier, linear amplifier. In this circuit, gain A and gain B amplifiers are balanced amplifiers. An output is sampled and the signal injected as inputs to gain A and gain B amplifiers.

- 5 There are two illustrated delays in the circuit shown in FIG. 1, delay N and delay B. Because the amplifiers are wideband, any delay compensates for the amplifiers. If the amplifiers are identical, then the delays are identical.

10 For purposes of the description of FIG. 1, the interconnection among various circuit components are described, followed by their function. Gain A amplifier **20** and Gain B amplifier **21** are balanced amplifiers. Gain A amplifier **20** connects to couplers DC1 **22** and DC2 **24** and to delay B circuit **26**, which series connects to couplers DC4 **28** and DC9 **30**. A radio frequency signal **32** enters through an attenuator **34** into the coupler DC8 **36** and into coupler DC1 **22**. The delay line, DelayS **38**, is coupled from coupler DC8 **36** and connects to coupler DC10 **40**. From coupler DC1 **22**, the signal passes to the gain A amplifier **20** into coupler DC2 **24**, as noted before. Series connected from the coupler DC4 **28** is the signal combination control circuitry **39a**, including diode detector **39**, analog-to-digital converter **40**, the power null circuit **42**, and the digital-to-analog converter **44**, which then passes signals to the AttB circuit **46**, the Phase B circuit **48**, coupler DC3 **49** and Gain B amplifier circuit **21**.

20 Coupler DC10 **40** also receives input signals via a delay line connected to coupler DC8 **36**, and coupler DC10 **40**. The signal passes from DC10 **40** as a detected signal into the distortion cancellation control circuitry **50a** having a diode D3 **50**, analog-to-digital converter **52**,

25

30

035033604467
032260

intermodulation distortion null circuit **54**, (IMD null), the digital-to-analog converter **56** and into the multiple carrier linear amplifier circuit segment shown generally by dotted line **58**.

5 The coupler DC1 **22** is connected into the delay A circuit **60** and into adjustment circuit **61**. In this embodiment, the adjustment circuit is an independent adjustment circuit **61** where phase and/or amplified signal components are independent. In other
10 embodiments, the phase and/or amplified signal components can be adjusted together. Thus, the invention can be accomplished independent or dependent (together). The circuit **61** includes coupler DC5 **62**, Delay N circuit **64**, AttB circuit **46** and Phase delay B circuit **48**, in series. The carrier null circuit **68**, as illustrated, includes a digital-to-analog converter circuit **70** and an analog-to-digital converter circuit **72** with DAC **70** connected to AttF circuit **74** and Phase F circuit **76**, coupling to DC5 **62** and coupler DC6 **78**,
15 which, in turn, connects to coupler DC2 **24**. Coupler DC7 **80** is ADC **72** connected and also connects to coupler DC6 **78**, diode **81**, and to 180 degree phase delay **82a** and phase shifter N circuit **82**, and series connected linear noise amplifier **84**, and AttN circuit **86** and DC3.
20

25 It should also be understood that the entire carrier cancellation line shown at **62**, **74**, **76** can be eliminated. The carrier and distortion would be adjusted at the coupler **89**. It is then possible to have an adjuster as the coupler at **89**, which adjusts
30 the phase and/or gain on both, i.e., the carrier and distortion. Thus, it is possible that the circuit could be used in other locations to detect other circuit functions, for example, to detect the carrier

0926200476 1032862

signal and the active sub-bands at the carrier null circuit **68**.

FIG. 1 shows the general block diagram of the amplifier architecture or system **18**, and includes a first amplifier path **87** and a second amplifier path **88** carrying replicas of signal components. On the first amplifier path **87**, the first amplifier **20** amplifies signal components and generates distortion components. A replica of the amplified signal components and distortion is provided to a coupling path **89**. The adjustment circuit **61** receives the distortion components from the coupling path **89** and the signal components from the second path **88** to independently adjust the phase and/or gain of at least one of the signal components and the distortion components, which adjusts the gain and/or phase relationship between the signal components and the distortion components. In this embodiment, the adjustment circuit **61** isolates the distortion components on the coupling path by combining signal components from the second path **88** and the signal components on the coupling path **89**, which are about 180 degrees out of phase and substantially equal in amplitude and thus canceled. The distortion components are amplitude and/or phase adjusted by the phase shifter **82** and the attenuator **86**. Because the signal components have been substantially removed from the coupling path, the phase and/or gain adjustments to the distortion components are made without a corresponding adjustment to the phase and/or amplitude of the signal components.

The adjusted distortion components are coupled onto the second path where the signal components and the adjusted distortion components are amplified by the second amplifier **21**. The amplified

02520146 02520262A

signal components and distortion components on the second path **88** are combined with the amplified signal components and distortion components on the first path **87** to combine constructively the signal components and 5 destructively combine the distortion components. In the embodiment of FIG. 1, using the illustrated independent adjustment circuit (although the circuit does not have to be independently adjusted), when the distortion components are adjusted relative to the 10 signal components, the phase and/or gain relationship between the signal components and the distortion components becomes independent. Thus, phase and/or gain adjustments to the distortion and signal components can be made, which improve both the 15 constructive combination of the signal components and the destructive combination of the distortion components.

In operation, the amplifier system **18**, the coupler **36**, such as a 10dB coupler (DC 8), receives the 20 signal RFin and couples replicas of the signal Rfin **32** onto the first amplifier path **87** and the second amplifier path **88** after an initial amplitude adjustment of RFin by the attenuator (AttIn) **34**. The coupler provides the signal components on the first path **87** 25 with 0 degrees phase shift and 10 dB of attenuation. The signal components are provided to the second path **88** with little attenuation and 90 degree of phase shift delay. The amplifier **20** amplifies the signal components on the first path by Gain A to produce the 30 amplified signal components along with distortion components generated by the amplifier with 0 degrees of relative phase shift. The coupler **24**, such as a 40 dB directional coupler, couples the signal components and the distortion components onto the first path **88** and

0536230145 002E83042

the coupling path **89**. Using a 40 dB coupler, the signal components and the distortion components are coupled onto the coupling path with 40 dB of attenuation with no phase shift. The signal components 5 and the distortion components remaining on the first path are delayed by a phase shift of 90 degrees with little attenuation to a phase value of -90 degrees. Further details of this type of circuit operation can be found in the incorporated by reference Hoffmann 2 10 patent application, U.S. patent application serial no. 09/564,321.

Distortion components isolated on the coupling path **89** are provided to a 180 degree phase delay **82a**, giving the distortion components on the 15 coupling path a phase value of 0 degrees (-180 -180 = -360 = 0 degrees). The phase shifter **82** provides a phase adjustment to the distortion components, which is not provided to the signal components which have been substantially canceled, reduced or removed from the 20 coupling path **89**. In this embodiment, the amplifier **84**, such as a low noise amplifier, amplifies the distortion components on the coupling path **89** by 26dB. The attenuator **86** provides an amplitude adjustment to the distortion components which is not provided to the 25 signal components which have been removed from the coupling path **89**. As such, the distortion components are phase and/or amplitude -adjusted independent of the signal components which have been substantially canceled, reduced or removed from the coupling path 30 prior to the distortion components being combined with signal components on the second path **88**. By independently phase and/or amplitude adjusting the distortion components on the coupling path **89**, the destructive combination of the corresponding distortion

00000000000000000000000000000000

components at the output of the amplifier architecture **18** can be independently controlled and improved.

In this circuit, in addition to making the relative gain and/or phase adjustments between the 5 distortion components independent of the relative phase and/or gain adjustments to the signal components, the signal components on the first path **87** become independent of the signal components on the second path **88**.

10 In other configurations where the power of the signal components is distributed among first and second amplifier paths, equal power at the inputs to first and second amplifiers on the separate paths can be achieved by sampling the output of the first
15 amplifier, rotating the phase of the sample, and attenuatively adding the sample to the signal components on the second path to reduce the level of the signal components through what can be referred to as vector attenuation. As such, the signal components
20 input to the second amplifier are dependent upon the output to the first amplifier.

The system **13** also distributes the power of the input signal components on the first and second amplifier paths **87,88**, thereby enabling improved power 25 efficiency. In this circuit, however, the signal components on the first path **87** are independent from the signal components on the second path **88**, for example, by passively coupling and attenuating the signal components on the second path without vector
30 attenuation. Because the signal components are removed from the coupling path **89**, the signal components on the second path **88** provided to the second amplifier **21** (GainB) are independent of the signal components output from the amplifier **20** (GainA) on the first path **87**, in

that the amplified signal components from the first amplifier **20** will not affect the signal components on the second path **88**. Additionally, the loss of the first amplifier **20** (GainA) will not result in an 5 undesired large increase in power level at the combined output of the system **18**. Instead, about one half of the power of the signal components would be produced.

The adjusted distortion components on the coupling path **89** are provided to the coupler **49**, such 10 as a 10dB directional coupler, which attenuates the distortion components on the coupling path **89** by about 10 dB and combines the distortion components from the coupling path with the signal components on the second path **88**. Before being provided to the coupler **49**, the 15 signal components from the coupler are delayed by the delay **64** (DelayN) by an amount such that the distortion components on the coupling path arrive at the coupler at substantially the same time as the signal components corresponding to the distortion components. The signal 20 components corresponding to the distortion components are the signal components which resulted in the distortion components when the signal components were amplified. The attenuator **46** adjusts the amplitude of the signal components on the second path **88**. A phase 25 delay **48**, such as a 90 degree phase delay, delays the signal components on the second path **88** by 90 degrees to have a phase value of -90 degrees. The attenuator **46** and the phase delay **48** provide gain and phase 30 adjustments to the signal components on the second path **88** without a corresponding change to the distortion components and thereby could be considered as part of an independent adjustment arrangement. The delay **64**, the attenuator **46** and the phase delay **48** provide constant time, amplitude and phase adjustments to

098620246 098620247

enable the different paths carrying components to be combined to match up in terms of time, gain and phase for improved combining given the components used in this embodiment.

5 The signal components on the second path **88** at -90 degrees and the adjusted distortion components on the coupling path **89** at 0 degrees are provided to the coupler **49**. In this embodiment, the coupler **49** phase shifts the signal components on the second path
10 **88** by 90 degrees to about -180 degrees and combines the signal components with the distortion components from the coupling path at about 0 degrees onto the second path. As such, the signal components with phase values at about -180 degrees and the distortion components
15 with phase values at about 0 degrees are provided onto the second path in this embodiment. However, the 180 degree out of phase relationship and/or the amplitude difference between the signal components and the distortion components on the second path **88** can be
20 changed due to the independent adjusting of the phase and/or amplitude of the distortion components on the coupling path **89**.

An attenuator **46** could adjust amplitude and the phase shifter **48** could shift the phase of the
25 signal and distortion components. The signal and distortion components are amplified by the amplifier **21**, and the amplified signal and distortion components are combined at the coupler **30**, such as a 3dB coupler, with the corresponding signal and distortion components
30 on the first path **87**. The amplifier **21** amplifies the distortion components received from the second path **88** at about 0 degrees and generates distortion components at about -180 degrees from amplifying the signal components from the second path **88** which are at -180

09876543210

degrees. In this circuit, the sampled distortion components from the amplifier **20** amplified by the amplifier **21** at about 0 degrees are reduced by the distortion components generated at the amplifier **21** at 5 about -180 degrees from amplifying the signal components at -180 degrees, leaving distortion components at about zero degrees.

In this circuit, the signal components at the input to the amplifier **21** should have the same 10 amplitude as the signal components at the amplifier **20** with a phase value of -180 degrees. The signal and distortion components from the coupler **28** at phase values of -90 degrees are provided to the delay **26** (DelayB) which delays the signal components and the 15 distortion components on the first path **87** such that the corresponding portions of the signal and distortion components on the first path **87** and the signal and distortion components on the second path **88** reach the coupler **30** at substantially the same time. The 20 amplified signal and distortion components on the first path **87** are received by the coupler **30**, which delays the signal and distortion components by 90 degrees to phase values of about -180 degrees. In producing the amplified signal components RFout, the coupler **30** 25 constructively combines the signal components from the first and second paths **87,88** in phase and at about the same amplitude such that the first and second paths each provide one-half of the power to the signal components at the output of the system. Since the 30 distortion components on the first and second paths **87,88** are at about 180 degrees out of phase, the distortion components on the first path destructively combine with the distortion components on the second

67
66
65
64
63
62
61
60
59
58
57
56
55
54
53
52
51
50
49
48
47
46
45
44
43
42
41
40
39
38
37
36
35
34
33
32
31
30
29
28
27
26
25
24
23
22
21
20
19
18
17
16
15
14
13
12
11
10
9
8
7
6
5
4
3
2
1
0

path to reduce the distortion components at the output of the coupler **30**.

As noted before, the independent adjustment circuit **61** enables the relative phase and/or gain between the distortion components on the first and second paths **87,88** to be adjusted independent of the relative phase and/or gain adjustments between the signal components on the first and second paths. It should be understood, however, as noted before, that the adjustment circuit **61** does not have to be independent but the phase and/or amplified signal components can be adjusted together. As such, the destructive combining of the distortion components from the first and second paths at the coupler **28** can be improved by performing adjustments to the relative phase and/or gain of the distortion component on the coupling path. The power amplifier system can also provide adjustable phase and/or amplitude adjustments to the signal components which do not result in a corresponding phase and/or amplitude adjustments to the distortion components to provide adjustment of the signal components.

The adjustment of the relative gain and/or phase of the distortion components and/or the signal components can be performed once to align the power amplifier architecture on the production line, periodically (based on changing conditions or expiration of a time period), or dynamically (based on changing operating conditions or continuously).

Because the constructive combination of the signal components can be made independent of the destructive combination of the distortion components, dynamic control to further improve the operation of the architecture can be provided in a relatively simple manner.

Coupler **78** can be used in conjunction with phase shifter **76** and attenuator **78** to improve cancellation of signal components. Dynamic control can also be provided by use of carrier null circuit **68** and
5 DAC circuit **70** and ADC circuit **72**, which work in conjunction with diode detector **81** and coupler **80**. The carrier null circuit **68** acts as a power detector with the diode detector **81** to provide a power signal, indicating how well the cancellation of the signal
10 components have been achieved.

Control circuitry can monitor the signal cancellation signal and provide control signals to the digital to analog (D/A) converter **70** to adjust the gain and/or phase provided by the gain **72** and phase
15 adjusters **74** in response to the signal cancellation signal. The control circuitry provides the control signals to find the gain and/or phase adjustments, which produce a null in the cancellation signal and reflects good cancellation of the signal components on
20 the coupling path **89**. This control can be set during initial alignment, or dynamic control provided. Dynamic control is provided because during operation any changes in the signal cancellation signal indicating a degradation in the cancellation of the
25 signal components on the coupling path **89** can be responded to with a control signal to adjust the gain and/or phase to improve cancellation of the signal components.

By achieving improved cancellation of the
30 signal components on the coupling path, the distortion components can be isolated on the coupling path, and the distortion components can be independently adjusted to improve the cancellation of the distortion components at the output of the coupler **28**. By

providing for adjustment of the distortion components, control of the combination of the distortion components is possible, and dynamic control of the cancellation of the distortion components can be readily achieved,
5 which in the presently illustrated circuit, are independently controlled.

A coupler **30** couples a replica of the output signal RFout onto a distortion cancellation path **90** and provides the signal to distortion cancellation control
10 circuitry **50a**, which provides gain and/or phase adjustment control signals to gain and/or phase adjusters **82,86** in response to the coupled output signal. A signal on the distortion cancellation path **90** is provided to the coupler **40**, which combines the
15 signal on the signal cancellation path with a delayed version of the signal components coupled from the coupler **36** at the input of the architecture. The signal components from the coupler **36** are delayed such that the corresponding portions of the signal
20 components arrive at the coupler **40** at substantially the same time. The corresponding signal components should be about 180 degrees out of phase such that the signal components are reduced and the distortion components from the signal on the distortion
25 cancellation path can be detected by detection circuitry **50**, for example including a diode detector.

The detection circuitry **50** provides a distortion cancellation signal indicating the level of the distortion components remaining on the output of
30 the coupler **28**, thereby indicating the level of the cancellation of the distortion components at the coupler **28**. The distortion cancellation signal is provided to an A/D converter **52**, which digitizes the distortion cancellation signal. The digitized

09320186 632280

distortion cancellation signal is provided to control circuitry **54**. The control circuitry **54** monitors the distortion cancellation signal and provides control signals to a digital to analog (D/A) converter **56** to adjust the gain and/or phase provided by the gain and phase adjusters in response to the distortion cancellation signal.

The control circuitry **54** provides the control signals to find the gain and/or phase adjustments which produce a null in the distortion cancellation signal which reflects good cancellation of the distortion components at the coupler **28**. This control can be set during initial alignment, or dynamic control provided. Dynamic control can be provided because, during operation, any changes in the distortion cancellation signal indicating a degradation in the cancellation of the distortion components at the coupler can be responded to with control signals to adjust the gain and/or phase to improve cancellation of the distortion components.

By providing for the adjustment of the distortion components, control over the constructive combination of the signal components at the coupler **28** is possible whereby gain and/or phase adjustments are made to the signal components (alone or together with the distortion components depending on the embodiment) depending on how the constructive combination of the signal components is performed. Dynamic control of the constructive combination of the signal components can be readily achieved. In this embodiment, a signal combination signal indicative of how well the signal components are combining in the coupler **28**, for example a signal on the isolated port of the coupler, is provided to signal combination control circuitry which

provides gain and/or phase adjustment control signals to gain and/or phase adjusters **46,48** in response to the signal combination signal.

The signal combination control circuitry
5 includes the detection circuitry **39**, for example including a diode detector, which detects the signal combination signal and provides a combination signal indicating how well the signal components combined in the coupler **28**. The combination signal is provided to
10 an A/D converter **40**, which digitizes the combination signal, and the digitized combination signal is provided to the power null, control circuitry **42**. The control circuitry **42** monitors the combination signal and provides control signals to a digital to analog
15 (D/A) converter **44** to adjust the gain and/or phase provided by any gain and phase adjusters **46,48** in response to the signal combination signal. The control circuitry **50a** provides the control signals to find the gain and/or phase adjustments which produce a null in
20 the combination signal which reflects good constructive combination of the signal components at the coupler. This control can be set during initial alignment, or dynamic control provided. Dynamic control is provided because, during operation, any changes in the signal
25 combination signal indicating a degradation in the combination of the signal components at the coupler can be responded to with control signals to adjust the gain and/or phase to improve constructive combination of the signal components.

30 In operation, it is evident that a signal is sampled and the main signal is cancelled because the coupler DC5 **62** samples the input and rotates it 180° . This circuit cancels from the sample and from the amplifier. What is left is the intermodulation

DRAFTS DRAFTS DRAFTS DRAFTS DRAFTS

distortion, and it is phase shifted, attenuated, and injected into the path of the other circuit signal into the gain B amplifier **21**, which amplifies the distortion. The input power to gain B amplifier **21** is
5 equal to the input power to gain A amplifier **20**, under most conditions. Because the gain B amplifier amplifies power as gain A, distortion will also be generated and combined with the amplified distortion.

As a result, the signal is combined with a
10 resultant, which will be equal in amplitude to the original distortion from the gain A amplifier, but 180° out of phase. When both distortions are added at coupler DC4 **28**, the distortions cancel each other. As will be suggested to those skilled in the art, there is
15 a question about the distortion left at the output for coupler DC9 **30**, which samples a combined total output signal and transfers the signal to coupler DC10 **40**. At the same time, the circuit samples the input from coupler DC8 **36** via the DelayS line **38**, which is applied
20 to the other side of coupler DC10 **40**. Both signals will be equal in amplitude and 180° out of phase and will cancel each other.

What will be cancelled will be the main signal, while at the inputs, there is no distortion.
25 What will be left after cancellation is the distortion product. Whatever power is left, the circuit will detect and digitize and send into the null circuit, which will provide adjustment as a closed loop until the null is minimized.

30 In order for this illustrated circuit to work properly, a large delay line is required, as shown with the line having DelayS **38**. The entire circuit is delayed. It is not desirable to have two different phase slopes, and thus, the delay is designed into the

circuit with DelayS line **38**. If there were two different phase slopes, then it would be necessary to cancel at coupler DC3. If there is no cancellation, then there would be a false indication of
5 intermodulation distortion and the circuit would not be aligned properly. It is known to those skilled in the art, however, if the delay is large, it is costly to design the circuit, and the circuit will be physically large. If the amplifier in this circuit is used in a
10 wideband configuration, such as with four different 20 MHz CDMA carriers in side-by-side relation, there will not be adequate cancellation.

FIG. 2 illustrates the improved circuit of the present invention using a pilotless intermodulation and quantization circuit **100** (IMD nullification circuit). In this circuit, no indication is taken from the inputs. Only the outputs are used and no delay line is necessary. The circuit of FIG. 2 is similar in structure and function to what is shown in FIG. 1, with
15 the exception of the added quantization circuit **100** of the present invention.
20

FIG. 3 is an enlarged schematic circuit diagram of the pilotless intermodulation distortion identification and quantization circuit **100** shown in FIG. 2. In this description, like elements from FIGS.
25 1 and 2 are described with common reference numerals.

In this circuit, there is a simulation of the multiple carrier linear amplifier circuit **101**, where the power comes in/out, and the drive passes into the
30 multiple carrier linear amplifier circuit. The control voltage is the same as in FIG. 2, and the upper coupler **102** is an equivalent for the coupler DC9, shown in FIG. 2.

Extending from the DC9 coupler equivalent **102** is an isolator **104**, which could be an optional circuit component. A synthesizer circuit **106** is coupled into a heterodyned mixer circuit **108**, which is series 5 connected to the isolator **104** and DC9 equivalent **102**. The synthesizer circuit **106** ensures that no leakage occurs back into the output of the amplifier system. The isolator **104** allows the power to drop, and it blocks those signals that would be prone to pass back 10 into the sample circuit corresponding to the DC9 equivalent **102**. The mixer circuit **108** functions similar to a small receiver.

The synthesizer circuit **106** includes a phase lock loop circuit **110** with phase **110a** and voltage **110b** 15 circuit components, and a loop filter corresponding to the operational amplifier **112** with the capacitive feedback using capacitor **114**. The phase lock loop circuit **110** connects to an oscillator circuit **116** and coupler circuit **118** with feedback from the coupler 20 circuit **118** for closed loop operation. A digital signal processor (DSP) circuit **120** connects to phase lock loop circuit **110** and allows intermodulation distortion and adjacent channel power (IMD/ACP) optimization control.

This DSP circuit **120** is a generic circuit and could be a microprocessor or other control circuit, as known to those skilled in the art. The DSP circuit **120** will determine, via an algorithm of the present invention, the frequency used to tune the synthesizer 25 circuit, which will generate the signal to be heterodyned for the output of the multiple channel linear amplifier. This signal is an intermediate frequency (IF) and passes to a low pass filter (LPF) **124**. The intermediate frequency (IF) is at a frequency 30

used for known standards, such as the DOCOMO/UMTS frequency plan. The low pass filter **124** eliminates any harmonics and images.

From the low pass filter **124**, the
5 intermediate frequency signal passes into the sample
and hold circuit **130**. The signal is received within a
bandpass filter (BPF) circuit **132** and will be a sharp
filter, similar to a saw filter. The signal is then
detected in a radio frequency detector **134**, which could
10 be any operable type known to those skilled in the art,
but in the present example, is a log detector. The
signal passes into a switch **136** and capacitor **138** that
together act as a sample and hold circuit. A timer
signal **140** is received from the DSP circuit **120** and
15 drives the overall circuit. The timing is selected for
best performance.

A stream of samples is received corresponding
to a DC signal representing the segments or "chunks" of
bandwidth. The DC signal will pass into the analog-to-
20 digital converter **142** and to DSP circuit **120**, where, in
accordance with the algorithm of the present invention,
processing occurs and decisions are based on the DC
signal level. From the DSP circuit **120**, the signal
passes into a digital-to-analog conversion circuit **144**
25 corresponding to DAC **56**, and then to the multiple
channel linear amplifier for phase shift and
attenuation.

The circuit shown in FIG. 3 is operative
based on the DOCOMO/UMTS frequency plan, where the RF
30 frequency range is 2110 to 2170 MHz. This overall band
is divided/designated into three sub-bands of 20 MHz
each. Each sub-band can handle up to four carriers of
5 MHz each. The total carriers per overall band are
twelve.

In summary of the operation, the synthesizer circuit **106** generates local oscillator (LO) frequencies, which are applied to the mixer circuit. A sampled MCLA output is applied to the RF side of the 5 mixer circuit **108**, as described before. The LO frequencies, in this example, are 2212.5 to 2267.5 MHz, 12 frequencies at 5 MHz increments, called $f_0, f_1 \dots f_{11}$. They are mixed with the sampled MCLA RF output. The mixing targets the centers of the 12 possible 10 carriers, at 2112.5 to 2167.5 MHz, which are also spaced at 5 MHz apart. The result is a fixed IF frequency, $f_{LO} - f_{RF} = 100$ MHz. The low pass filter will eliminate the $f_{LO} + f_{RF}$ products.

The resulting IF signal passes through the 15 band pass filter **132**, which is centered at 100 MHz, having a passband of ~3 MHz. The filtered RF is applied to the log detector **134** and the sample and hold (S&H) circuit **136**, as described before, where it is digitized by the analog-to-digital conversion circuit 20 (quantization) **142**. The algorithm presented in FIG. 10 will optimize and null the intermodulation distortion, as described below. As noted before, the algorithm is described and shown relative to the W-CDMA DOCOMO/UMTS frequency plan. There are 12 possible carriers 25 available across the band.

Relative to FIG. 10, which will be described in detail later, the basic algorithm determines active sub-bands and based on those active sub-bands, the circuit determines where the intermodulation distortion 30 settings will be placed. Although this depends on the sub-bands, this is an implementation specific circuit. Once the intermodulation distortion settings are set, the local oscillator frequency (LO) is set such that the intermodulation distortion settings are typically

next to the active sub-bands. Then the intermodulation distortion is reduced based on those measurements at that point.

IS-95 PCS is also 60 MHz wide, but carrier-to-carrier spacing is 1.5 MHz, which yields a total of 48 possible carriers. In reality, only 46 are available, as two carriers are not valid because of bandwidth limitations at the band edges. IS 95 also has six designated sub-bands, three 15 MHz, and three 5 MHz each.

For IS-136, TDMA, the frequency plan is different. Carrier to carrier spacing is only 30 kHz, but a group of up to 15 carriers is used simultaneously per sector. This pattern yields a total band of 450 kHz per sector, or roughly 0.5 MHz. Any bandpass filter in the hardware circuit will be matched per application, as well as the number of frequency steps and perhaps some logic in the algorithm.

In one aspect of the present invention, as a non-limiting example, fRF = 2112.5 to 2167.5 MHz, 12 carriers at 5 MHz BW each, divided into three sub-bands of 20 MHz with four carriers. (Overall RF range is 2110 to 2170 MHz.)

fLO = 2212.5 to 2267.5 MHz, 12 frequencies at 5 MHz increments, called F0, f1 . . . f11.

fIF = 100 MHz.

FIGS. 4-9 are bar charts illustrating the three sub-bands of 20 MHz each, where each sub-band handles up to four carriers of 5 MHz. The adjacent channel power (ACP) and alternate adjacent channel power (AACP) graph blocks are illustrated. FIG. 10 illustrates a flow chart for the basic algorithm used with the circuit shown in FIGS. 2 and 3.

It is shown from the flow chart that an initial sweep is made of the various frequencies. As

is described above in greater detail, the synthesizer
is stepped up and there are 12 different frequencies.
The data coming out of the channels will have a DC
voltage that has been digitized to represent the signal
5 strength of the power coming out of the respective
channel. As shown in FIG. 4, the first signal carrier
represents an actual carrier. Frequencies 5, 6, 8 and
9 are equivalent frequencies out of the twelve
frequencies at issue. This represents the
10 intermodulation product.

As shown in FIG. 5, the two frequency blocks
are side-by-side. The spaced 5 MHz spectral signals
are represented by frequencies 4, 5, 8 and 9. FIGS. 6
and 7 illustrate two carriers that are spaced 10 and 15
15 MHz apart respectively, but still within the single
sub-band.

FIGS. 8 and 9 illustrate a worse case
indication having four different levels with four
carriers maximum per sector. FIG. 9 illustrates the 50
20 channels where the Delta P (ΔP) equals 17dB max from
"pilot only" to all 50 channels. If there is a working
system and all carriers are "on", the maximum
difference the system can expect from a fully loaded
carrier to the pilot is about 17°. The numbers can
25 change from system to system. It is evident from the
description that the synthesizer circuit sweeps a
scheme, and it is possible to download to the processor
as many algorithms as desired.

FIG. 10 illustrates a flow chart for the
30 algorithm that is applicable for use with the circuits
shown in FIGS. 2 and 3.

As noted before, the algorithm as shown in
FIG. 10 determines active sub-bands and based on those
active sub-bands determines where the intermodulation
35 distortion setting will be placed. After this, the

local oscillator is set such that the intermodulation distortion setting would be next to the active sub-bands. The intermodulation distortion is then reduced based on the measurements at that point. Thus,
5 based on the active sub-bands, the local oscillator is set to the intermodulation distortion. Based on these active sub-bands, it is possible to know where the intermodulation distortion is located and the IMD can be detected and cancelled.

10 For example, in the flow chart, which will be described in greater detail later, at block **204**, the twelve outputs are compared and the system scans the twelve increments. Each one is looked at based on a threshold (such as if it is above a certain decibel level). If it is above that threshold, then it is an active sub-band and a determination is made as in **206a**,
15 **206b**, **206c**, whether certain sub-bands are active. If not active, then the IMD settings are retained, as at block **208**. Throughout this description, $F(Lo)$ equals
20 the local oscillator frequency and $F(x)$ equals the lowest active carrier frequency within a sub-band. $F(X+N)$ equals N frequency above the lowest, while $F(low)$ equals the inactive carrier frequency when any three out of four carriers are active.

25 For example, if F_0 to F_3 is active, such as at decision block **206a**, then the system determines which of all four are on. If all four carriers are on, then for example, the local oscillator frequency is set to $F(X+4)$. The different settings for different
30 examples are shown in the figures shown in FIGS. 4-9, if the four carriers are on and $F(X+4)$ is not an active sub-band, but next to it is the intermodulation distortion and that will be reduced. Thus, the sub-bands are identified at any increment, which is
35 above a certain threshold. That is considered an

C-20230414-A-022233-E

active sub-band after the process is followed through as in the flow chart of FIG. 10.

Depending on those active sub-bands, the circuit determines via the algorithm how to set the local oscillator to the IMD desired. For example, if all four sub-bands are "on," the system determines that it is at the high end of the spectrum. If the system goes higher, it is out of band. Thus, it is necessary to set the IMD to $F(X-1)$, i.e., the next lowest increment below the band where the highest IMD will be located. If any three carriers are on, then the system moves to the inactive carrier frequency out of the group of four and to the one that is inactive where the IMD will be located. For example, $F(X)$, $F(X+1)$ can be the two lowest carriers, and thus, the local oscillator is set to $F(X-1)$. The IMD will be located adjacent to it. This is shown in FIGS. 4, 5, 6 and 7. Thus, depending on the active sub-band, the system places the local oscillator at the spot and that is where the IMD will be at. There are, of course, different combinations as set forth in FIGS. 4-10. It is desirable not to go into another carrier's band.

The process starts and the circuit steps the LO from F_0 to F_{11} , as indicated at block 200. The detector output is recorded, corresponding to the DC signal coming out (block 202) and the 12 outputs are compared to identify the sub-band (block 204). This occurs by determining sub-band A, sub-band B or sub-band C and determining which frequencies, such as F_0 to F_3 , are active in blocks 206a, 206b and 206c, through appropriate decision making. If none of the frequencies are active, then the intermodulation distortion settings are retained (block 208). This initial sweep identifies a sub-band. It is not possible to sweep the sub-band only to determine

DRAFT PAGES 1-20 OF 20

additional frequencies out-of-band, where one would expect the adjacent channel power (ACP) to be high enough and detectable. Once it is determined that a sub-band is active, decisions are made as to the
5 carriers that are active. It is not necessary to step once again because it is loaded in memory and a threshold is set.

For example, if sub-band A or B is active (block 210), then decisions are made to check whether
10 all four carriers are on (power equals high) (block 212), any three carriers are on (block 214), any two carriers are on and the spacing (blocks 216, 218 and 220), or whether one carrier is on (block 222). If yes, then the results are shown at blocks 224, 226,
15 228, 230, 232 and 234. The system tests for null (block 236) and adjusts the respective intermodulation distortion controls, the attenuation and phase circuits (block 238). The settings are saved (block 240), and if the null is less than the threshold (block 242),
20 then the stepping procedure begins once again (block 200).

If sub-band C is active (Block 244), corresponding to frequencies F8 to F11, then a determination is made whether all four carriers are on
25 (block 246), any three carriers are on (block 248), any two carriers are on with different separation (blocks 250, 252 or 254), or only one carrier is on (block 256). If yes, then the local oscillator frequency is adjusted as indicated at blocks 258, 260, 262, 264, 266
30 or 268 respectively. Then the test is made for null at block 236.

It is evident from this flowchart that the digital signal processor circuit will set the control voltage and start searching. It will adjust the
35 attenuation and phase shift until minimization occurs

and there is a null. In this description, $F(x)$ and $F(x+1)$ corresponds to adjacent carriers while $F(x+3)$ corresponds to 15 MHz separation.

Many modifications and other embodiments of
5 the invention will come to the mind of one skilled in
the art having the benefit of the teachings presented
in the foregoing descriptions and the associated
drawings. Therefore, it is to be understood that the
invention is not to be limited to the specific
10 embodiments disclosed, and that the modifications and
embodiments are intended to be included within the
scope of the dependent claims.

DRAFTING CO. INC. - 6325 3rd Ave